



# MP2328C

High-Efficiency, 28V, 2A, 450kHz,  
Synchronous Step-Down Converter  
with PG, SS, and Forced CCM

## DESCRIPTION

The MP2328C is a fully integrated, high-frequency, synchronous, rectified, step-down switch-mode converter with internal power MOSFETs. It offers a very compact solution to achieve 2A of continuous output current ( $I_{OUT}$ ) across a wide input voltage ( $V_{IN}$ ) range, with excellent load and line regulation. The MP2328C offers synchronous mode operation for high efficiency across the wide  $I_{OUT}$  load range.

Constant-on-time (COT) control provides very fast transient response and easy loop design, as well as tight output regulation.

Full protection features include short-circuit protection (SCP), over-current protection (OCP), under-voltage protection (UVP), and thermal shutdown.

The MP2328C requires a minimal number of readily available, standard external components. It is available in a space-saving SOT583 package.

## FEATURES

- Wide 4.5V to 28V Operating Input Voltage ( $V_{IN}$ ) Range
- Wide 0.5V to 16V Output Voltage ( $V_{OUT}$ ) Range
- $\pm 1.5\%$  Internal Reference Accuracy Over-Temperature (OT)
- 130m $\Omega$ /60m $\Omega$  Low  $R_{DS(ON)}$  Internal Power MOSFETs
- >92% Efficiency for 24V to 5V/2A Condition
- Fast Load Transient Response
- 450kHz Switching Frequency ( $f_{SW}$ )
- $t_{ON}$  Extension to Improve Dropout
- Configurable Soft-Start Time ( $t_{SS}$ )
- Forced Continuous Conduction Mode (FCCM)
- Power Good (PG) Indication
- Over-Current Protection (OCP) with Hiccup Mode
- Thermal Shutdown Protection
- Available in a SOT583 Package



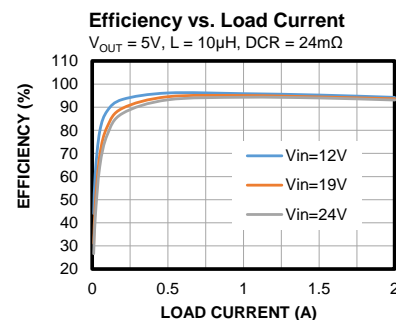
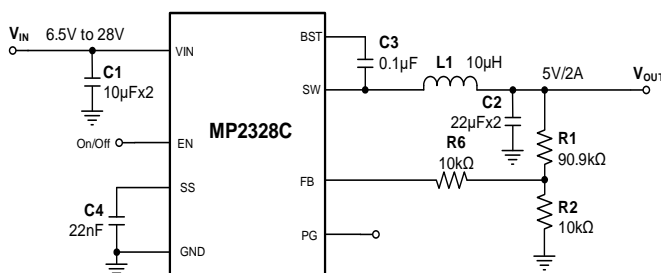
Optimized Performance with  
MPS Inductor MPL-AL6060 Series

## APPLICATIONS

- Game Consoles
- Multi-Function Printers
- Power Meters
- Flat-Panel Televisions and Monitors
- General-Purpose Power Supplies

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## TYPICAL APPLICATION



### ORDERING INFORMATION

Part Number*	Package	Top Marking	MSL Rating
MP2328CGTL	SOT583	See Below	1

\* For Tape & Reel, add suffix -Z (e.g. MP2328CGTL-Z).

### TOP MARKING

**BRNY**

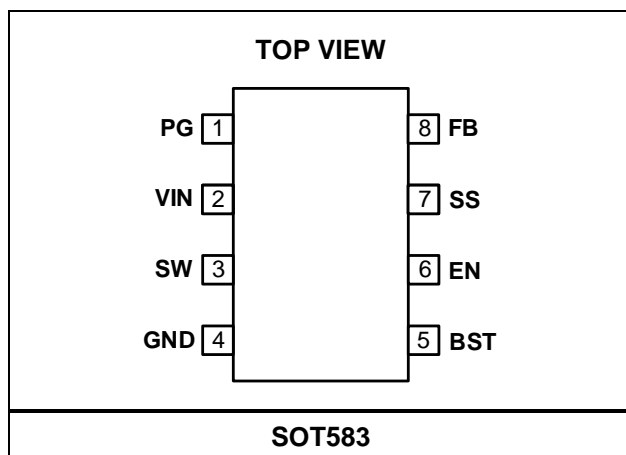
**LLL**

BRN: Product code of MP2328CGTL

Y: Year code

LLL: Lot number

### PACKAGE REFERENCE



## PIN FUNCTIONS

Pin #	Name	Description
1	PG	<b>Power good output.</b> This pin is an open-drain output. When the IC is disabled, PG is pulled low. PG can be pulled up to other DC source. Note that if PG is pulled up to an external voltage, then it does not de-assert (logic low) when the input power is off. It is recommended to pull PG up to the output voltage ( $V_{OUT}$ ) so that PG can de-assert (logic low) when the input power is off.
2	VIN	<b>Supply voltage.</b> The MP2328C operates from a 4.5V to 28V input rail. Place a capacitor on VIN to decouple the input rail. Connect VIN using a wide PCB trace.
3	SW	<b>Switch output.</b> Connect SW using a wide PCB trace.
4	GND	<b>System ground.</b> Reference ground of the regulated $V_{OUT}$ . GND requires careful consideration when designing the PCB layout. Connect GND with copper traces and vias.
5	BST	<b>Bootstrap.</b> Connect a capacitor between the SW and BST pins to form a floating supply across the high-side MOSFET (HS-FET) driver. It is typically recommended to use a 0.1 $\mu$ F bootstrap capacitor.
6	EN	<b>Enable pin.</b> EN is a digital input that turns the buck regulator on and off. When the power supply of the control circuit is ready, pull EN high to turn the buck regulator on. Pull EN low to turn the regulator off. Connect EN to VIN through a voltage resistor divider for automatic start-up. The EN voltage should not exceed 6V.
7	SS	<b>Soft start.</b> Connect an external capacitor to SS to configure the soft-start time ( $t_{SS}$ ) for the switch-mode regulator.
8	FB	<b>Feedback.</b> Connect FB to the tap of an external resistor divider from the output to GND to set $V_{OUT}$ .

### ABSOLUTE MAXIMUM RATINGS <sup>(1)</sup>

$V_{IN}$ .....	-0.3V to +30V
$V_{SW}$ .....	-0.3V (-5V for <10ns) to +30V (32V for <10ns)
$V_{BST}$ .....	$V_{SW} + 5.5V$
All other pins .....	-0.3V to +6V
PG pin current .....	5mA <sup>(2)</sup>
Continuous power dissipation ( $T_A = 25^\circ C$ ) <sup>(3)</sup>	2.27W <sup>(4)</sup>
Junction temperature .....	150°C
Lead temperature .....	260°C
Storage temperature .....	-65°C to +150°C

### ESD Ratings

Human body model (HBM) .....	$\pm 2000V$
Charged device model (CDM) .....	$\pm 750V$

### Recommended Operating Conditions <sup>(5)</sup>

Supply voltage ( $V_{IN}$ ) .....	4.5V to 28V
Output voltage ( $V_{OUT}$ ) .....	0.5V to 0.95 x $V_{IN}$ or 16V max
Operating junction temp ( $T_J$ ) ....	-40°C to +125°C

### Thermal Resistance

	$\theta_{JA}$	$\theta_{JC}$
SOT583		
EVL2328C-TL-00A <sup>(4)</sup> .....	55 .....	21°C/W
JESD51-7 <sup>(6)</sup> .....	130 .....	60°C/W

#### Notes:

- Exceeding these ratings may damage the device.
- When the PG pin is pulled up to power source, the current should be limited below the maximum value.
- The maximum allowable power dissipation is a function of the maximum junction temperature  $T_J$  (MAX), the junction-to-ambient thermal resistance,  $\theta_{JA}$ , and the ambient temperature,  $T_A$ . The maximum allowable continuous power dissipation at any ambient temperature is calculated by  $P_D$  (MAX) =  $(T_J$  (MAX) -  $T_A$ ) /  $\theta_{JA}$ . Exceeding the maximum allowable power dissipation can generate excessive die temperature, which may cause the regulator to go into thermal shutdown. Internal thermal shutdown circuitry protects the device from permanent damage.
- Measured on the EVL2328C-TL-00A, 2-layer PCB (63.5mmx63.5mm).
- The device is not guaranteed to function outside of its operating conditions.
- The value of  $\theta_{JA}$  given in this table is only valid for comparison with other packages and cannot be used for design purposes. These values were calculated in accordance with JESD51-7 and simulated on a specified JEDEC board. They do not represent the performance obtained in an actual application.

## ELECTRICAL CHARACTERISTICS

$V_{IN} = 12V$ ,  $T_J = -40^{\circ}C$  to  $+125^{\circ}C$ , typical values are tested at  $T_J = 25^{\circ}C$ , the over-temperature (OT) limit is derived by characterization, unless otherwise noted. <sup>(7)</sup>

Parameter	Symbol	Condition	Min	Typ	Max	Units
<b>Power Supply</b>						
$V_{IN}$ under-voltage lockout (UVLO) threshold	$V_{IN\_UVLO\_R}$	$V_{IN}$ rising, $V_{EN} = 2V$	3.66	3.96	4.25	V
$V_{IN}$ UVLO hysteresis	$V_{IN\_UVLO\_HYS}$			330		mV
Shutdown supply current	$I_{SD}$	$V_{EN} = 0V$		2	10	$\mu A$
Quiescent supply current	$I_Q$	$V_{EN} = 2V$ , $V_{FB} = 0.55V$		560	700	$\mu A$
<b>Enable Control</b>						
EN rising threshold	$V_{EN\_RISE}$		1.1	1.2	1.3	V
EN hysteresis	$V_{EN\_HYS}$			120		mV
EN input current	$I_{EN}$	$V_{EN} = 2V$		2	10	$\mu A$
<b>Power MOSFET</b>						
High-side MOSFET (HS-FET) on resistance	$HS_{RDS\_ON}$	$V_{BST\_SW} = 5V$		130		m $\Omega$
Low-side MOSFET (LS-FET) on resistance	$LS_{RDS\_ON}$			60		m $\Omega$
Switch leakage	$SW_{LKG}$	$V_{EN} = 0V$			1	$\mu A$
<b>Current Limit</b>						
Low-side (LS) switching valley current limit	$I_{LIMIT\_LS\_OC}$		1.9	2.75	3.6	A
Negative current limit	$I_{NEG}$	$V_{OUT} = 5V$ , $L = 1.5\mu H$		-1.6		A
<b>Frequency</b>						
Oscillator frequency	$f_{SW}$	$V_{IN} = 12V$ , $V_{OUT} = 5V$ , $I_{OUT} = 1.5A$	350	450	550	kHz
Minimum on time <sup>(8)</sup>	$t_{ON\_MIN}$			50		ns
Minimum off time <sup>(8)</sup>	$t_{OFF\_MIN}$			160		ns
<b>Feedback Control</b>						
Feedback (FB) voltage	$V_{REF}$	$T_J = 25^{\circ}C$	495	500	505	mV
		$T_J = -40^{\circ}C$ to $+125^{\circ}C$	492.5	500	507.5	mV
FB current	$I_{FB}$	$V_{FB} = 0.5V$		10	50	nA
Soft-start current	$I_{SS}$		5.5	7.5	9.5	$\mu A$

**ELECTRICAL CHARACTERISTICS (continued)**

$V_{IN} = 12V$ ,  $T_J = -40^{\circ}C$  to  $+125^{\circ}C$ , typical values are tested at  $T_J = 25^{\circ}C$ , the over-temperature (OT) limit is derived by characterization, unless otherwise noted. <sup>(7)</sup>

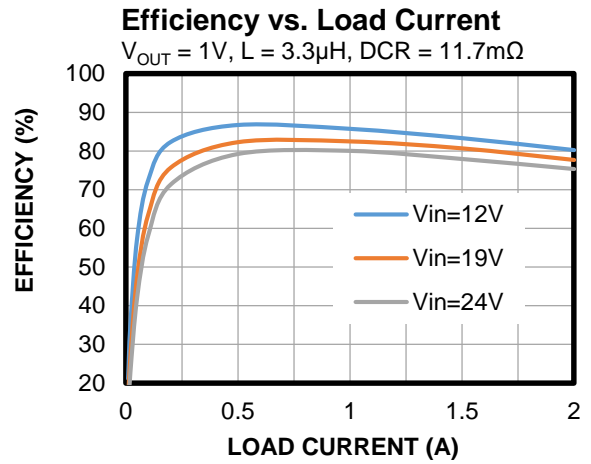
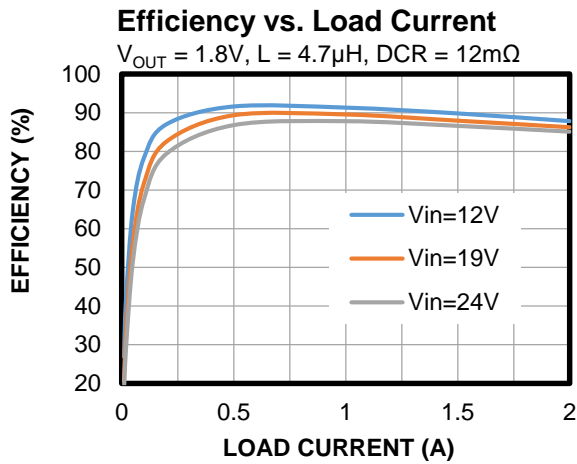
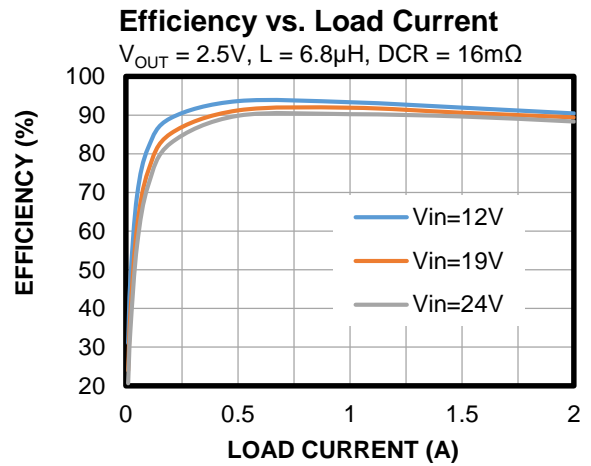
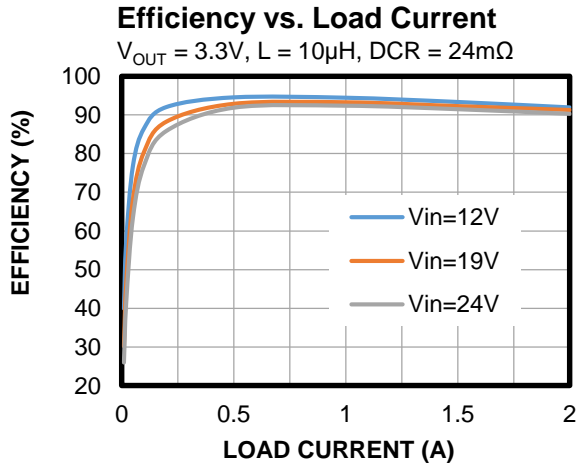
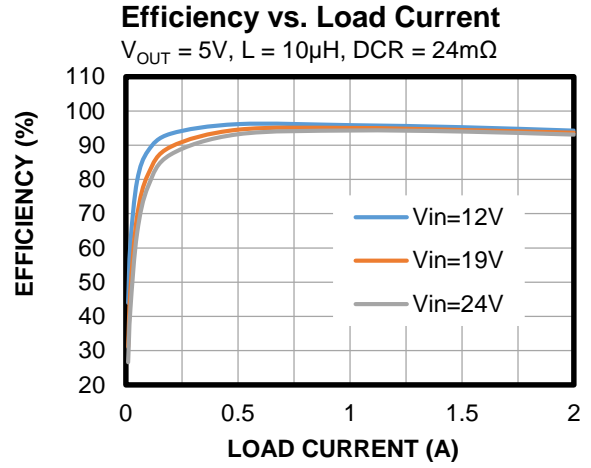
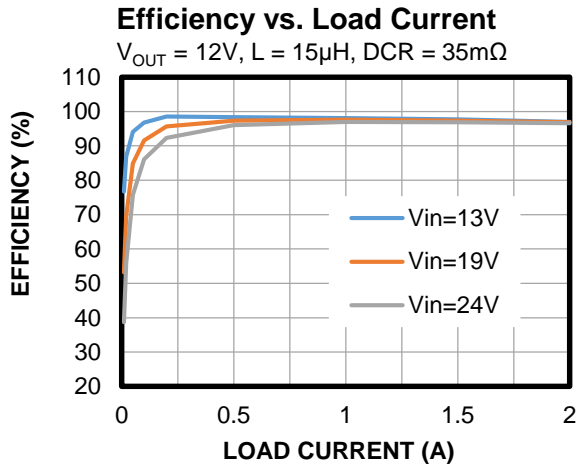
Parameter	Symbol	Condition	Min	Typ	Max	Units
<b>Power Good (PG) Indication</b>						
PG lower trip rising threshold	PG <sub>LOWER-R</sub>	PG from low to high	85	90	95	% of $V_{REF}$
PG lower trip falling threshold	PG <sub>LOWER-F</sub>	PG from high to low	79	84	89	% of $V_{REF}$
PG upper trip rising threshold	PG <sub>UPPER-R</sub>	PG from high to low	107	112	117	% of $V_{REF}$
PG upper trip falling threshold	PG <sub>UPPER-F</sub>	PG from low to high	101	106	111	% of $V_{REF}$
PG rising delay	PG <sub>TD-R</sub>			12		$\mu s$
PG falling delay	PG <sub>TD-F</sub>			20		$\mu s$
PG sink current capability	$V_{PG}$	Sink 4mA			0.4	V
PG leakage current	$I_{PG-LKG}$	$V_{IN} = 12V$ , $V_{EN} = 2V$ , $V_{FB} = 0.52V$ , $V_{PG} = 5V$		2	10	$\mu A$
<b>Protection</b>						
FB under-voltage (UV) threshold	FBUV <sub>VTH</sub>		40	50	60	% of $V_{REF}$
Hiccup protection duty cycle <sup>(8)</sup>	D <sub>HICCUP</sub>			25		%
Thermal shutdown	T <sub>SD</sub>			150		$^{\circ}C$
Thermal shutdown hysteresis	T <sub>SD-HYS</sub>			20		$^{\circ}C$

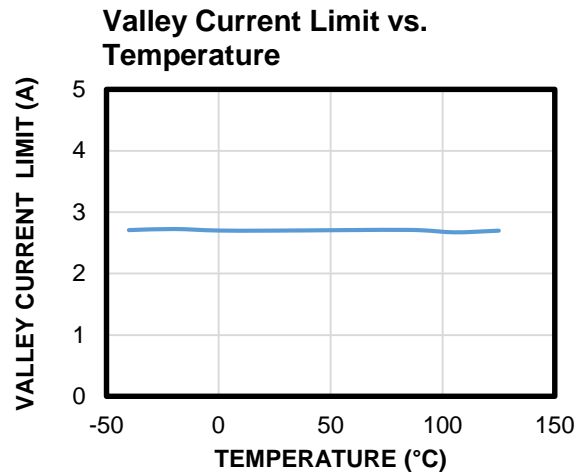
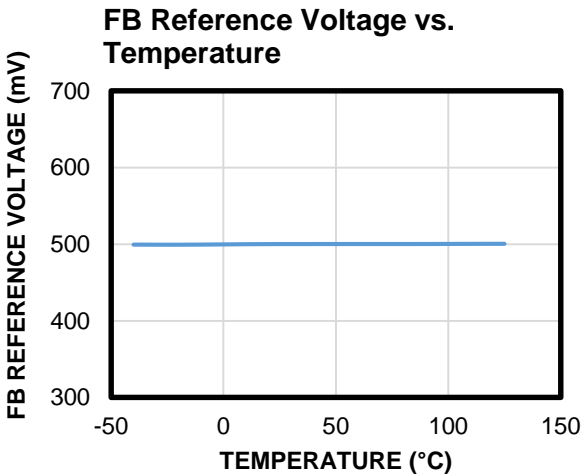
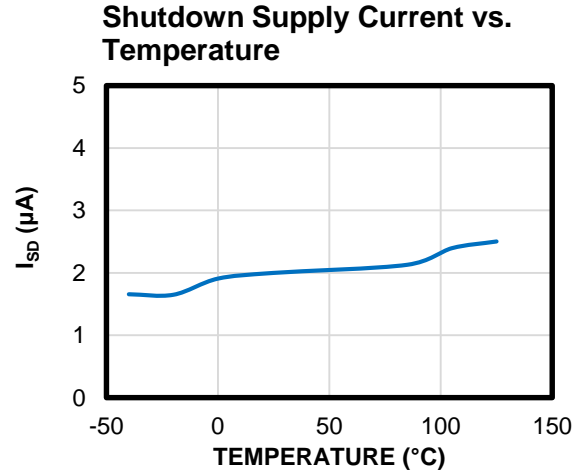
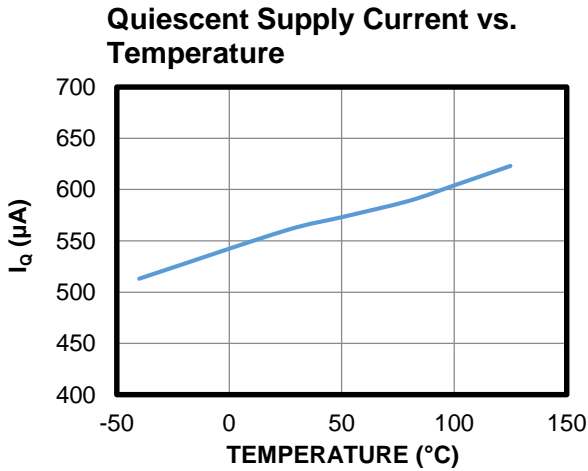
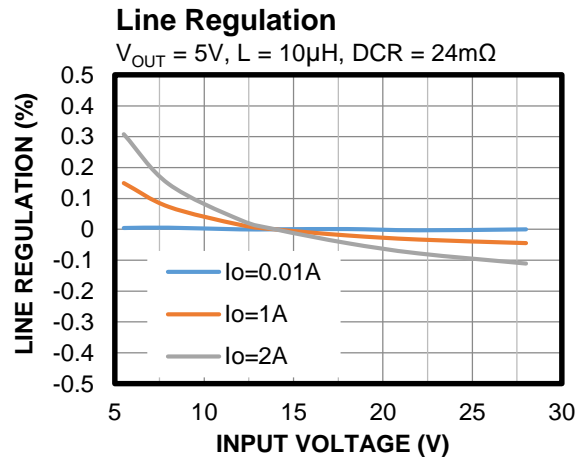
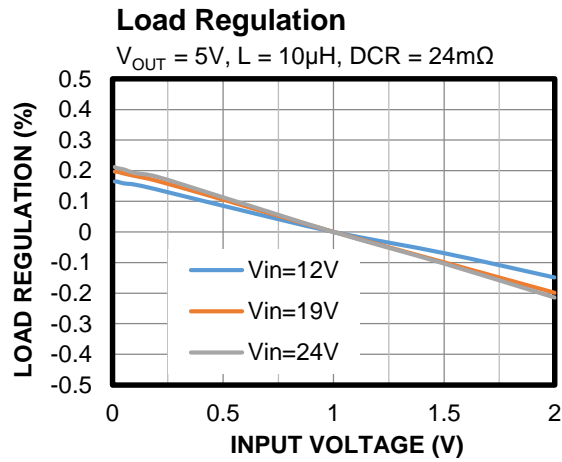
**Notes:**

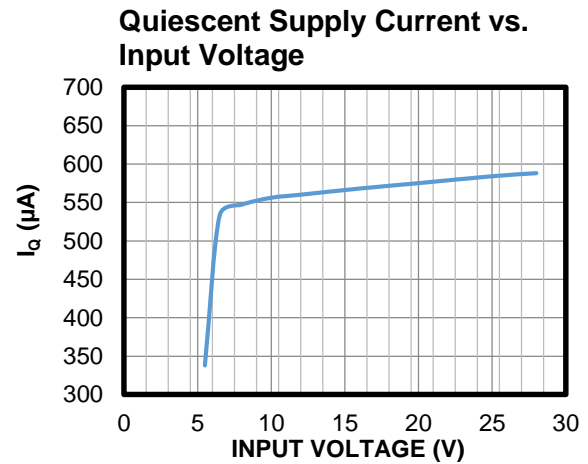
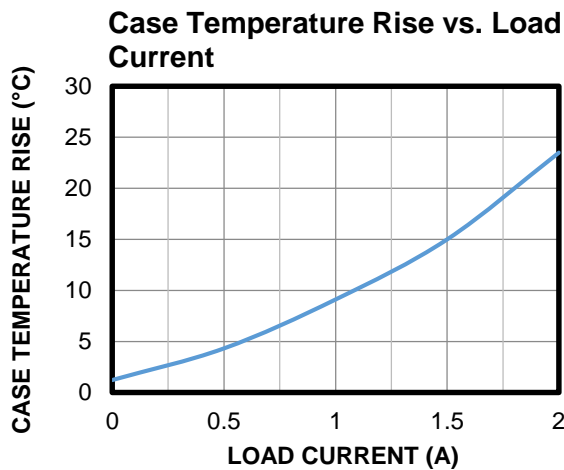
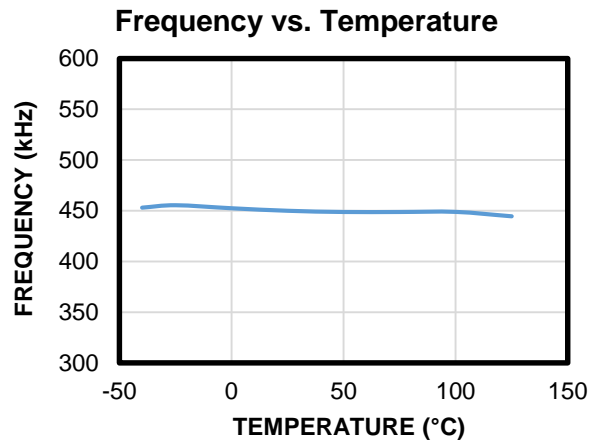
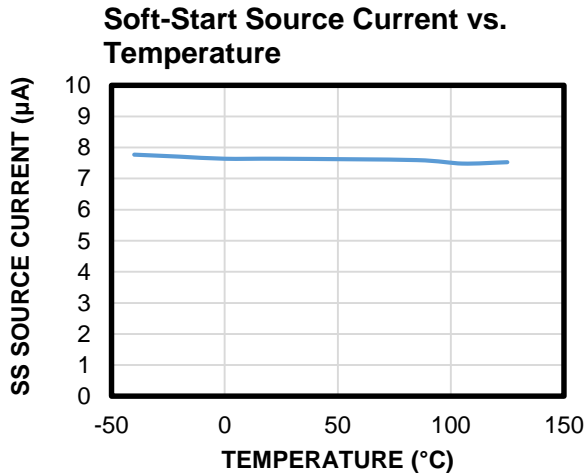
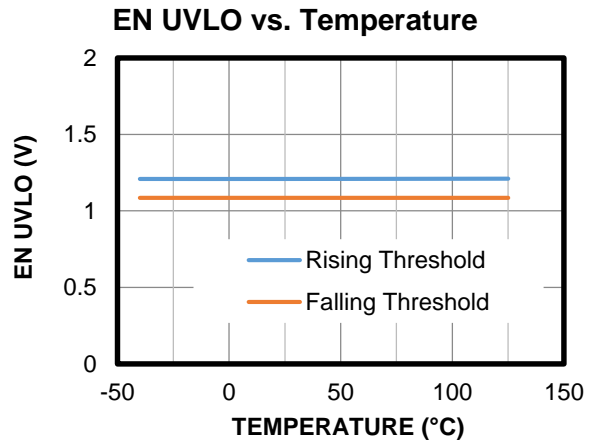
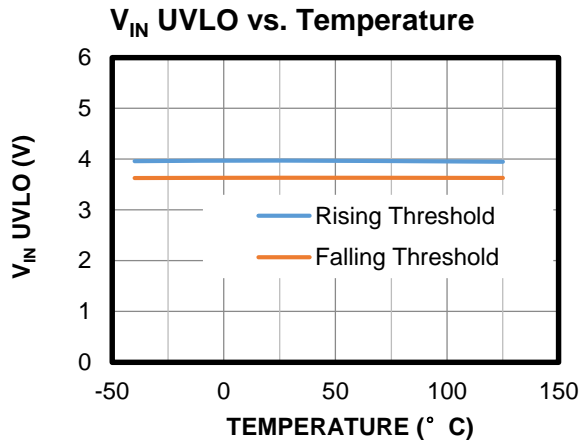
- 7) Not tested in production. Derived by over-temperature correlation.  
 8) Derived by sample characterization. Not tested in production.

## TYPICAL CHARACTERISTICS

$V_{IN} = 12V$ ,  $V_{OUT} = 5V$ ,  $L = 10\mu H$ ,  $T_A = 25^\circ C$ , unless otherwise noted.



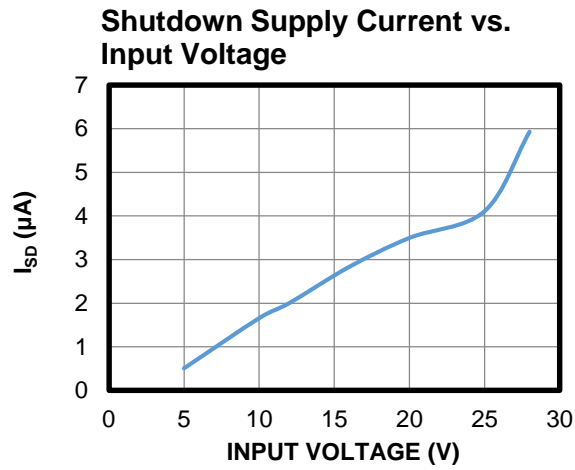
**TYPICAL CHARACTERISTICS (continued)**
 $V_{IN} = 12V, V_{OUT} = 5V, L = 10\mu H, T_A = 25^\circ C$ , unless otherwise noted.


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 $V_{IN} = 12V$ ,  $V_{OUT} = 5V$ ,  $L = 10\mu H$ ,  $T_A = 25^\circ C$ , unless otherwise noted.




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$V_{IN} = 12V$ ,  $V_{OUT} = 5V$ ,  $L = 10\mu H$ ,  $T_A = 25^\circ C$ , unless otherwise noted.

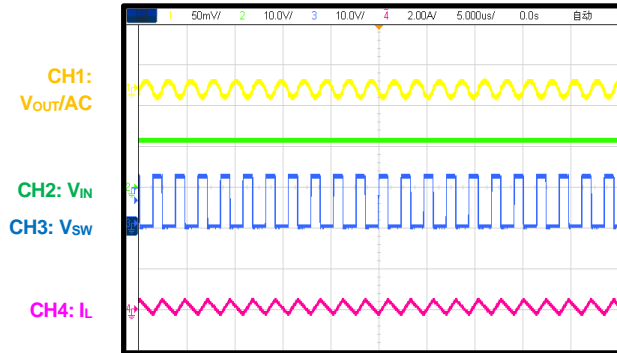


## TYPICAL PERFORMANCE CHARACTERISTICS

$V_{IN} = 12V$ ,  $V_{OUT} = 5V$ ,  $L = 10\mu H$ ,  $T_A = 25^\circ C$ , unless otherwise noted.

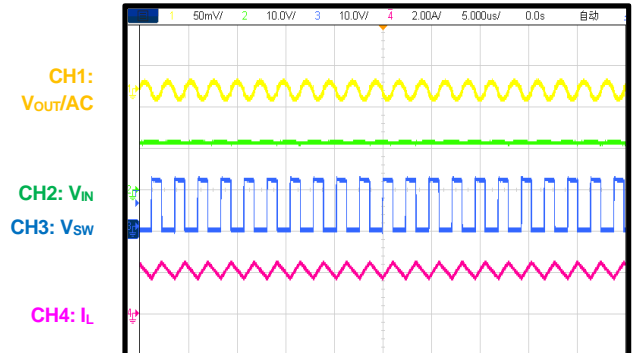
### Steady State

$I_{OUT} = 0A$



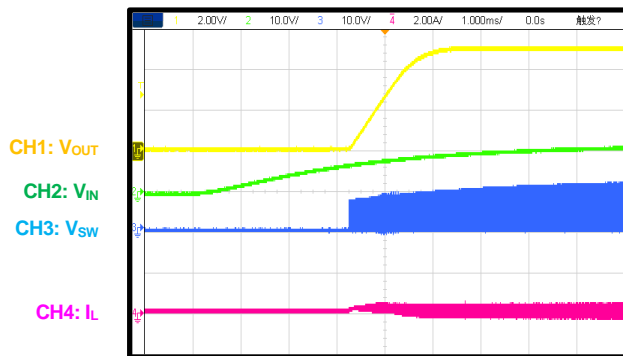
### Steady State

$I_{OUT} = 2A$



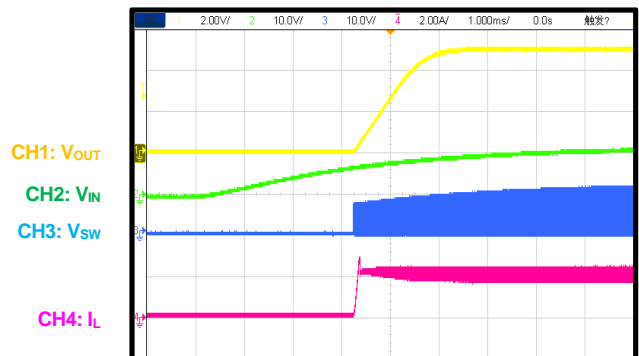
### Input Power Start-Up

$I_{OUT} = 0A$



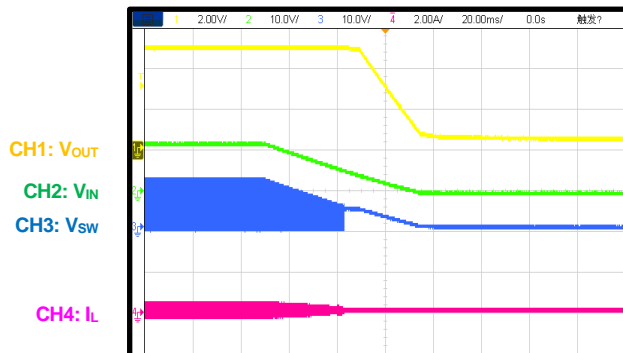
### Input Power Start-Up

$I_{OUT} = 2A$



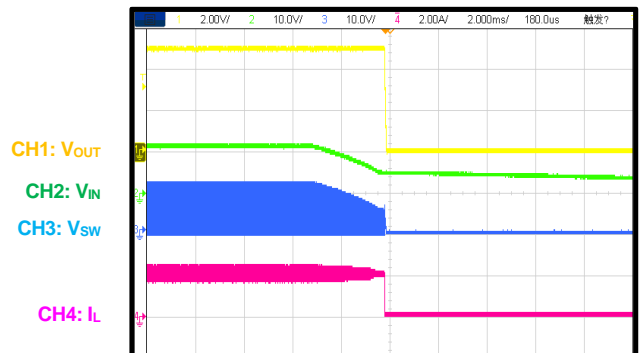
### Input Power Shutdown

$I_{OUT} = 0A$



### Input Power Shutdown

$I_{OUT} = 2A$

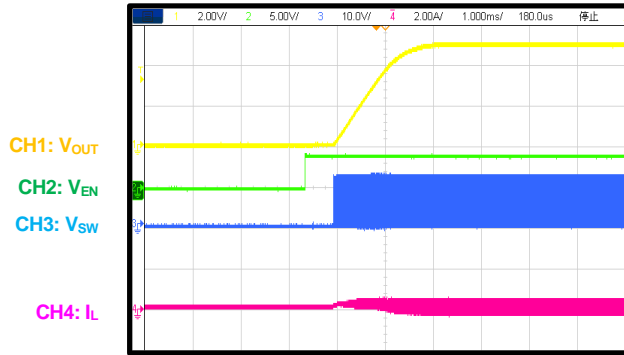


## TYPICAL PERFORMANCE CHARACTERISTICS (continued)

$V_{IN} = 12V$ ,  $V_{OUT} = 5V$ ,  $L = 10\mu H$ ,  $T_A = 25^\circ C$ , unless otherwise noted.

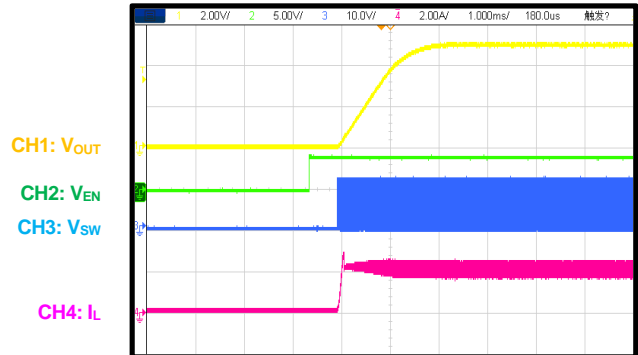
### Start-Up through EN

$I_{OUT} = 0A$



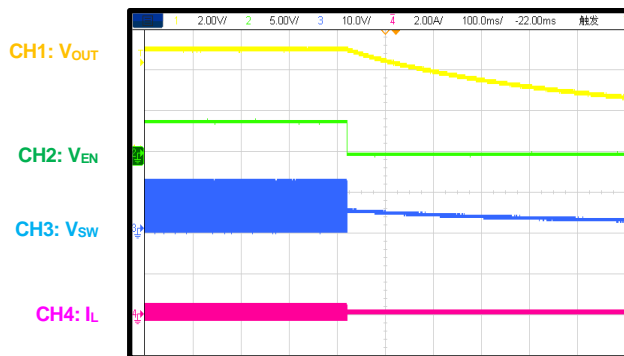
### Start-Up through EN

$I_{OUT} = 2A$



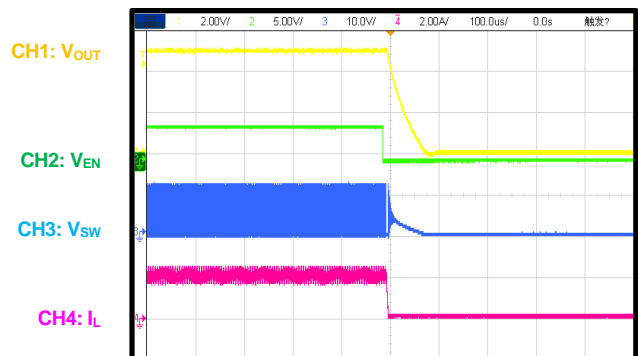
### Shutdown through EN

$I_{OUT} = 0A$



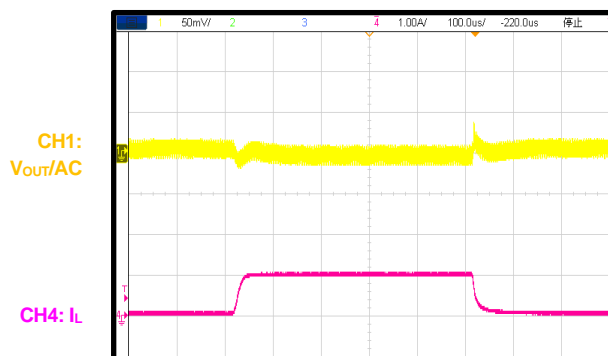
### Shutdown through EN

$I_{OUT} = 2A$



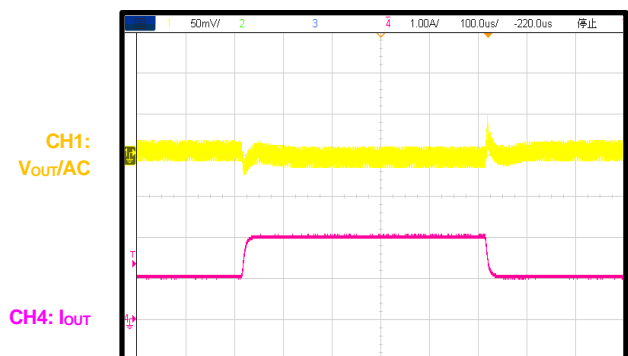
### Load Transient

$I_{OUT} = 0A$  to  $1A$

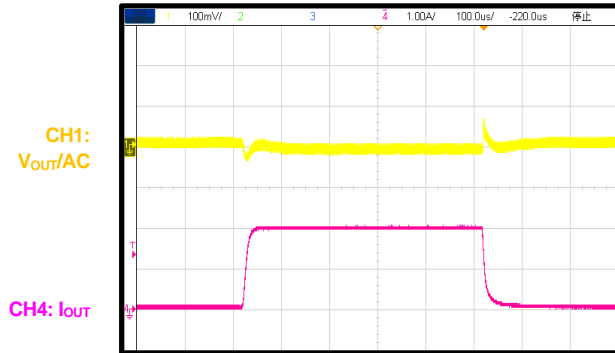
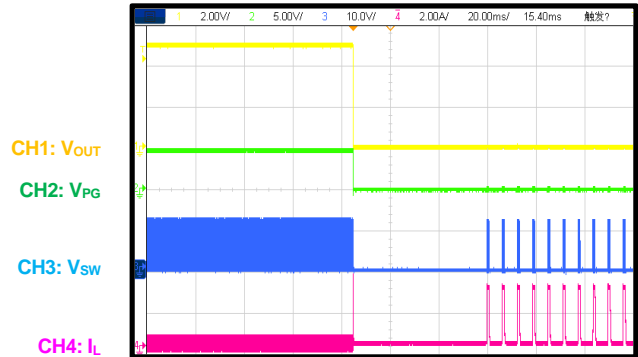
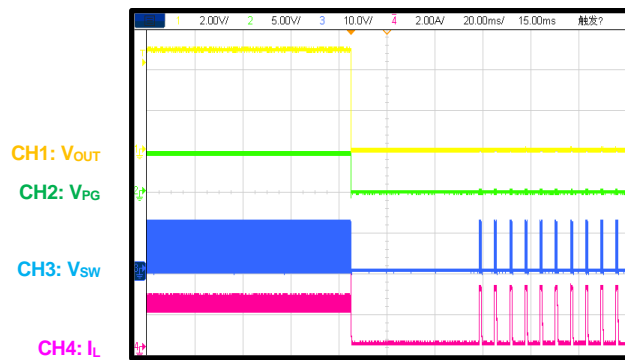
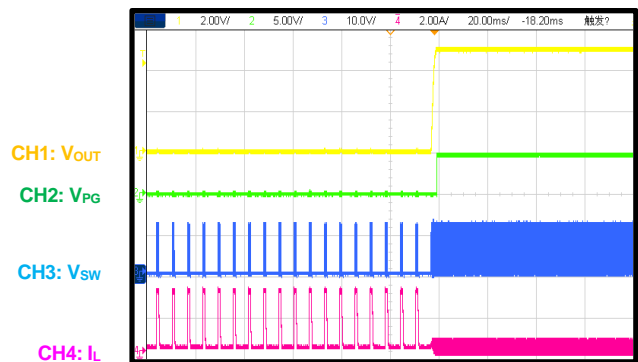
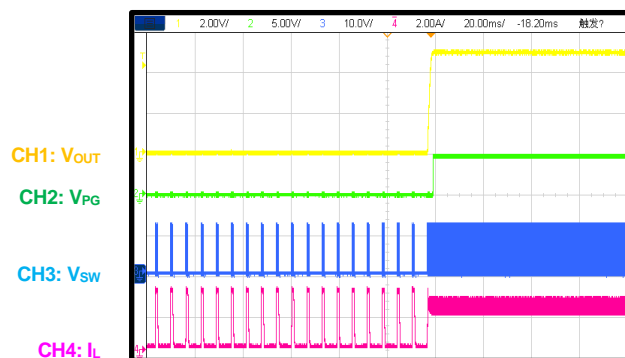


### Load Transient

$I_{OUT} = 1A$  to  $2A$



**TYPICAL PERFORMANCE CHARACTERISTICS (continued)**
 $V_{IN} = 12V, V_{OUT} = 5V, L = 10\mu H, T_A = 25^\circ C$ , unless otherwise noted.

**Load Transient**
 $I_{OUT} = 0A \text{ to } 2A$ 

**SCP Entry**
 $I_{OUT} = 0A$ 

**SCP Entry**
 $I_{OUT} = 2A$ 

**SCP Recovery**
 $I_{OUT} = 0A$ 

**SCP Recovery**
 $I_{OUT} = 2A$ 


## FUNCTIONAL BLOCK DIAGRAM

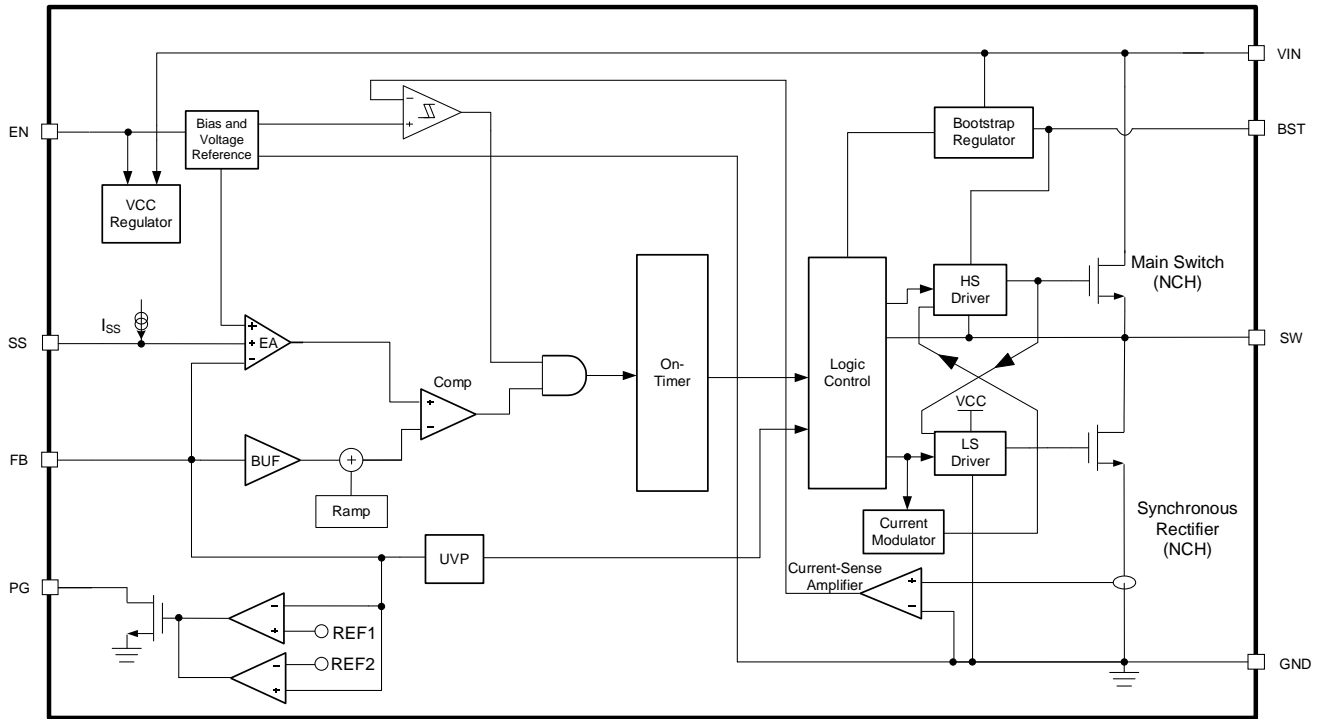


Figure 1: Functional Block Diagram

## OPERATION

### Pulse-Width Modulation (PWM) Operation

The MP2328C is a fully integrated, synchronous, rectified, step-down switch-mode converter. Constant-on-time (COT) control is employed to provide fast transient response and ease loop stabilization.

At the beginning of each cycle, the high-side MOSFET (HS-FET) turns on when the FB voltage ( $V_{FB}$ ) drops below the reference voltage ( $V_{REF}$ ). The HS-FET turns on for a fixed interval, determined by the one-shot on timer. The on-timer is determined by both the output voltage ( $V_{OUT}$ ) and input voltage ( $V_{IN}$ ) to keep the switching frequency ( $f_{SW}$ ) fairly constant across the  $V_{IN}$  range. After the on period finishes, the HS-FET turns off until the next period begins. By repeating this operation, the converter regulates  $V_{OUT}$ .

The low-side MOSFET (LS-FET) turns on when the HS-FET is off to minimize conduction loss. If both the HS-FET and LS-FET turn on at the same time, a dead short occurs between the input and GND. This is called shoot-through. To prevent shoot-through, a dead time (DT) is generated internally between the HS-FET off time and LS-FET on time, and vice versa.

The MP2328C works in forced continuous conduction mode (FCCM) to achieve smaller output ripple, better load regulation, and improved transient response in full load range.

### Enable (EN) Control

The enable (EN) pin can enable or disable the entire chip. Pull EN high to turn the regulator on; pull it low to turn the regulator off.

For automatic start-up, EN can be pulled up to  $V_{IN}$  through a voltage resistor divider. There is an internal  $1M\Omega$  resistor from EN to GND. To calculate the automatic start-up voltage ( $V_{IN\_START}$ ), determine the values of the pull-up resistor ( $R_{UP}$ , from  $V_{IN}$  to EN) and pull-down resistor ( $R_{DOWN}$ , from EN to GND) using Equation (2):

$$V_{IN\_START} = 1.3 \times \frac{R_{UP} + R_{DOWN} // 1000k\Omega}{R_{DOWN} // 1000k\Omega} \quad (1)$$

For example, if  $R_{UP} = 191k\Omega$  and  $R_{DOWN} = 49.9k\Omega$ , set  $V_{IN\_START}$  to 6.5V.

To avoid damaging the internal circuit, the EN voltage must not exceed 6V.

### Under-Voltage Lockout (UVLO)

$V_{IN}$  under-voltage lockout (UVLO) protects the chip from operating at an insufficient supply voltage. The UVLO rising threshold is about 3.96V, and its falling threshold is about 3.63V typically.

### Soft Start (SS)

The MP2328C employs a soft start (SS) mechanism to ensure smooth output ramping during start-up.

When the part starts, an internal current source (typically  $7.5\mu A$ ) charges up the SS capacitor ( $C_{SS}$ ) to generate a soft-start voltage ( $V_{SS}$ ).

When  $V_{SS}$  is below  $V_{REF}$ ,  $V_{SS}$  overrides  $V_{REF}$ . The error amplifier (EA) uses  $V_{SS}$  as the reference, and  $V_{OUT}$  ramps up smoothly. Once  $V_{SS}$  exceeds  $V_{REF}$ , the EA uses  $V_{REF}$  as the reference. At this point, soft start finishes and the device enters steady state operation.

$C_{SS}$  can be determined using Equation (2):

$$C_{SS} (nF) = \frac{t_{SS} (ms) \times I_{SS} (\mu A)}{V_{REF}} \quad (2)$$

### Over-Current Protection (OCP)

The MP2328C has a valley current limit. While the LS-FET is on, the inductor current is monitored. When the sensed inductor current ( $I_L$ ) reaches the valley current limit, the LS limit comparator (see Figure 1 on page 13) turns over and the device enters over-current protection (OCP) mode. The HS-FET does not turn on again until the valley current limit disappears. Meanwhile,  $V_{OUT}$  drops until  $V_{FB}$  falls below the FB under-voltage (UV) threshold. Once a UV condition is triggered, the MP2328C enters hiccup mode (after SS) to periodically restart the part.

During OCP, the device tries to recover from the over-current (OC) fault with hiccup mode. In hiccup mode, the chip disables the output power stage, discharges the soft-start capacitor, and then automatically tries to soft start again. If the OC condition remains after SS ends, then the device repeats this operation cycle until the OC

conditions disappear, and the output rises back to the regulation level.

### Power Good (PG)

The power good (PG) pin indicates whether  $V_{OUT}$  is in the normal range compared to the internal  $V_{REF}$ . It is an open-drain output that requires an external pull-up supply. During start-up, the PG output is pulled low, which indicates to the system to remain off and keep the load on the output to a minimum. This helps reduce inrush current at start-up.

When  $V_{OUT}$  is between 90% and 112% of the internal  $V_{REF}$  and SS is finished, the PG signal is pulled high. If  $V_{OUT}$  is below 84% after SS finishes, the PG signal stays low.

When  $V_{OUT}$  exceeds 112% of the internal  $V_{REF}$ , PG switches low. The PG signal is pulled high once  $V_{OUT}$  drops below 106% of the internal reference voltage.

The PG output is pulled low when EN UVLO, OCP, or over-temperature protection (OTP) is triggered.

If PG is pulled up to an external voltage, then PG does not de-assert (logic low) when  $V_{IN}$  drops below 0.8V. If PG is pulled up to  $V_{OUT}$ , then PG de-asserts (logic low) when  $V_{IN}$  drops below 0.8V.

### On Time ( $t_{ON}$ ) Extension

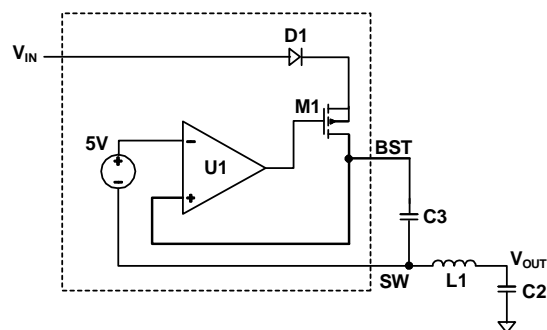
To improve dropout, the MP2328C is designed to extend its on time ( $t_{ON}$ ) when the duty cycle exceeds 92%. When the HS-FET on time is extended, the frequency drops. The typical minimum frequency is 250kHz. The frequency cannot drop below 250kHz.

### Pre-Biased Start-Up

The MP2328C is designed for monotonic start-up into pre-biased loads. If the output is pre-biased to a certain voltage during start-up, the bootstrap (BST) voltage ( $V_{BST}$ ) is refreshed and charged. The voltage on the soft-start capacitor is also charged. If  $V_{BST}$  exceeds its rising threshold voltage and  $V_{SS}$  exceeds the sensed output feedback voltage at the FB pin, the part starts switching normally.

### Floating Driver and Bootstrap Charging

An external BST capacitor ( $C_{BST}$ ) powers the floating power MOSFET driver. This floating driver has its own UVLO protection, with a 2.62V rising threshold and a 130mV hysteresis.  $V_{IN}$  regulates the  $C_{BST}$  voltage internally through D1, M1, C3, L1, and C2 (see Figure 2). If ( $V_{IN} - V_{SW}$ ) exceeds 5V, then U2 regulates M1 to maintain a 5V  $V_{BST}$  across C3.



**Figure 2: Internal Bootstrap Charger**

### Start-Up and Shutdown

If both  $V_{IN}$  and EN exceed their respective thresholds, the chip starts up. The reference block starts first, generating stable  $V_{REF}$  and currents, and then the internal regulator is enabled. The regulator provides a stable supply for the remaining circuits.

Three events can shut down the chip: EN low,  $V_{IN}$  low, and thermal shutdown. The shutdown procedure begins by blocking the signaling path to avoid any fault triggering. Then the internal supply rail is pulled down.

### Thermal Shutdown

Thermal shutdown prevents the chip from operating at exceedingly high temperatures. When the silicon die temperature exceeds 150°C, the entire chip shuts down. When the temperature falls below its lower threshold (typically 130°C), the chip is enabled again and resumes normal operation.

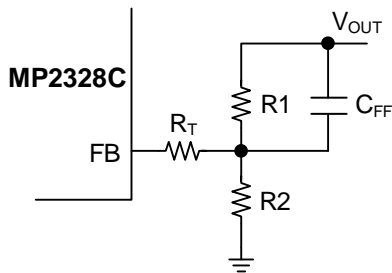
## APPLICATION INFORMATION

### Setting the Output Voltage

The external resistor divider sets  $V_{OUT}$ . First, choose a value for R2. R2 should be chosen reasonably, as a small R2 value results in considerable quiescent current loss, while a large R2 value makes the FB noise sensitive. It is recommended to set R2 to be between 5k $\Omega$  and 50k $\Omega$  for a good balance between system stability and no-load loss. R1 can then be calculated using Equation (3):

$$R1 = \frac{V_{OUT} - V_{REF}}{V_{REF}} \times R2 \quad (3)$$

Figure 3 shows the feedback circuit.  $R_T$  is an optional resistor for feedback compensation.



**Figure 3: Feedback Network**

Table 1 lists the recommended parameters for common output voltages.

**Table 1: Parameter Selection for Common Output Voltages**

$V_{OUT}$ (V)	R1 (k $\Omega$ )	R2 (k $\Omega$ )	$R_T$ (k $\Omega$ )	$C_{FF}$ (pF)	L ( $\mu$ H)
1	51	51	10	82	3.3
1.8	51	19.6	10	470	4.7
2.5	51	12.7	10	470	6.8
3.3	51	9.09	10	470	10
5	90.9	10	10	300	10
12	255	11	10	82	15

### Selecting the Inductor

The inductor supplies constant current to the output load while being driven by the switched  $V_{IN}$ . A larger-value inductor results in less ripple current and a lower output ripple voltage; however, it also has a larger physical footprint, higher series resistance, and lower saturation current. The inductance can be calculated using Equation (4):

$$L = \frac{V_{OUT}}{f_{sw} \times \Delta I_L} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right) \quad (4)$$

Where  $\Delta I_L$  is the peak-to-peak inductor ripple current.

The inductor should not saturate under the maximum peak inductor current. The peak inductor current can be calculated using Equation (5):

$$I_{LP} = I_{OUT} + \frac{V_{OUT}}{2 \times f_{sw} \times L} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right) \quad (5)$$

MPS inductors are optimized and tested for use with our complete line of integrated circuits.

Table 2 lists our power inductor recommendations. Select a part number based on the relevant design requirements.

**Table 2: Power Inductor Selection**

Part Number	Inductance	Manufacturer
MPL-AL	2.2 $\mu$ H to 15 $\mu$ H	MPS
MPL-AL-6050-3R3	3.3 $\mu$ H	MPS
MPL-AL-6060-4R7	4.7 $\mu$ H	MPS
MPL-AL6060-6R8	6.8 $\mu$ H	MPS
MPL-AL6060-100	10 $\mu$ H	MPS
MPL-AL6060-150	15 $\mu$ H	MPS

Visit [MonolithicPower.com](http://MonolithicPower.com) under Products > Inductors for more information.

### Selecting the Input Capacitor

The step-down converter has a discontinuous input current, and requires a capacitor to supply the AC current to the converter while maintaining the DC input voltage. Ceramic capacitors are recommended for the best performance, and should be placed as close to the  $V_{IN}$  pin as possible. Capacitors with X5R and X7R ceramic dielectrics are recommended because they are fairly stable amid temperature fluctuations.

The capacitors must also have a ripple current rating exceeding the maximum input ripple current of the converter. The input ripple current ( $I_{CIN}$ ) can be estimated using Equation (6):



$$I_{CIN} = I_{OUT} \times \sqrt{\frac{V_{OUT}}{V_{IN}} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right)} \quad (6)$$

The worst-case condition occurs at  $V_{IN} = 2 \times V_{OUT}$ , which can be estimated using Equation (7):

$$I_{CIN} = \frac{I_{OUT}}{2} \quad (7)$$

For simplification, choose an input capacitor with an RMS current rating that exceeds half of the maximum load current.

The input capacitance determines the input voltage ripple ( $\Delta V_{IN}$ ) of the converter. If there is a  $\Delta V_{IN}$  requirement in the system, choose the input capacitor that meets the relevant specifications.

$\Delta V_{IN}$  can be estimated using Equation (8):

$$\Delta V_{IN} = \frac{I_{OUT}}{f_{sw} \times C_{IN}} \times \frac{V_{OUT}}{V_{IN}} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right) \quad (8)$$

Under worst-case conditions where  $V_{IN} = 2 \times V_{OUT}$ ,  $\Delta V_{IN}$  can be estimated using Equation (9):

$$\Delta V_{IN} = \frac{1}{4} \times \frac{I_{OUT}}{f_{sw} \times C_{IN}} \quad (9)$$

### Selecting the Output Capacitor

The output capacitor ( $C_{OUT}$ ) is required to maintain the DC output voltage. Ceramic or POSCAP capacitors are recommended. The output voltage ripple ( $\Delta V_{OUT}$ ) can be estimated using Equation (10):

$$\Delta V_{OUT} = \frac{V_{OUT}}{f_{sw} \times L} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right) \times \left(R_{ESR} + \frac{1}{8 \times f_{sw} \times C_{OUT}}\right) \quad (10)$$

With ceramic capacitors, the capacitance dominates the impedance at  $f_{sw}$ , and causes the majority of  $\Delta V_{OUT}$ . For simplification,  $\Delta V_{OUT}$  can be estimated using Equation (11):

$$\Delta V_{OUT} = \frac{V_{OUT}}{8 \times f_{sw}^2 \times L \times C_{OUT}} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right) \quad (11)$$

$\Delta V_{OUT}$  caused by the ESR is very small. With POSCAP capacitors, the ESR dominates the impedance at  $f_{sw}$ . For simplification,  $\Delta V_{OUT}$  can be estimated using Equation (12):

$$\Delta V_{OUT} = \frac{V_{OUT}}{f_{sw} \times L} \times \left(1 - \frac{V_{OUT}}{V_{IN}}\right) \times R_{ESR} \quad (12)$$

Besides considering the output ripple, choosing a larger-value  $C_{OUT}$  improves load transient response, but the maximum  $C_{OUT}$  limit should also be considered in design applications. If  $C_{OUT}$  is too high,  $V_{OUT}$  cannot reach the design value during the soft-start time and fails to regulate. The maximum  $C_{OUT}$  value ( $C_{O\_MAX}$ ) can be limited using Equation (13):

$$C_{O\_MAX} = (I_{LIM\_AVG} - I_{OUT}) \times t_{SS} / V_{OUT} \quad (13)$$

Where  $I_{LIM\_AVG}$  is the average start-up current during SS, and  $t_{SS}$  is the soft-start time.

### Design Example

Table 3 is a design example following the application guidelines for the specifications below.

**Table 3: Design Example**

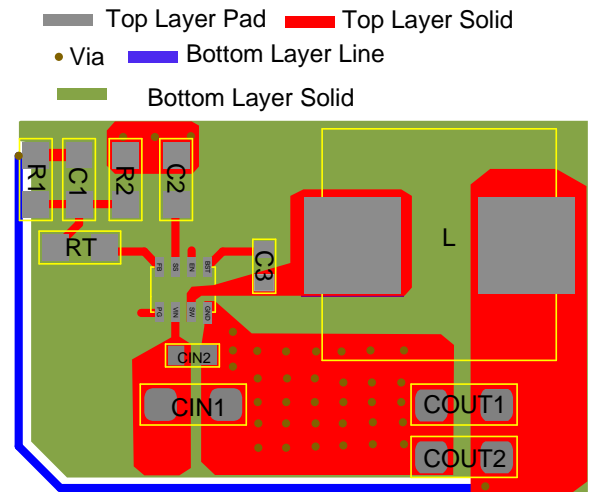
$V_{IN}$	$V_{OUT}$	$I_{OUT}$
6.5V to 28V	5V	2A

For the detailed application schematic, see Figure 9 on page 20. For the typical performance and circuit waveforms, see the Typical Performance Characteristics section on page 10. For more device applications, refer to the related evaluation board datasheet.

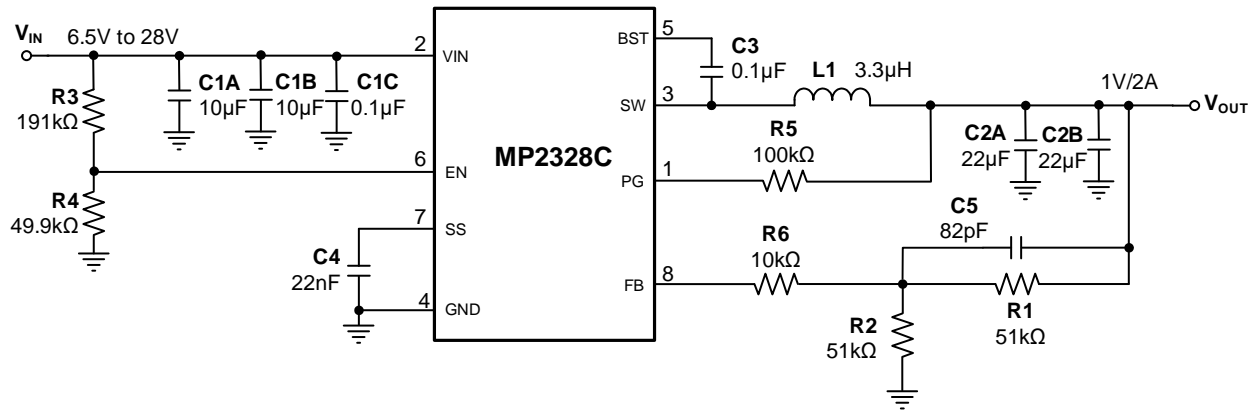
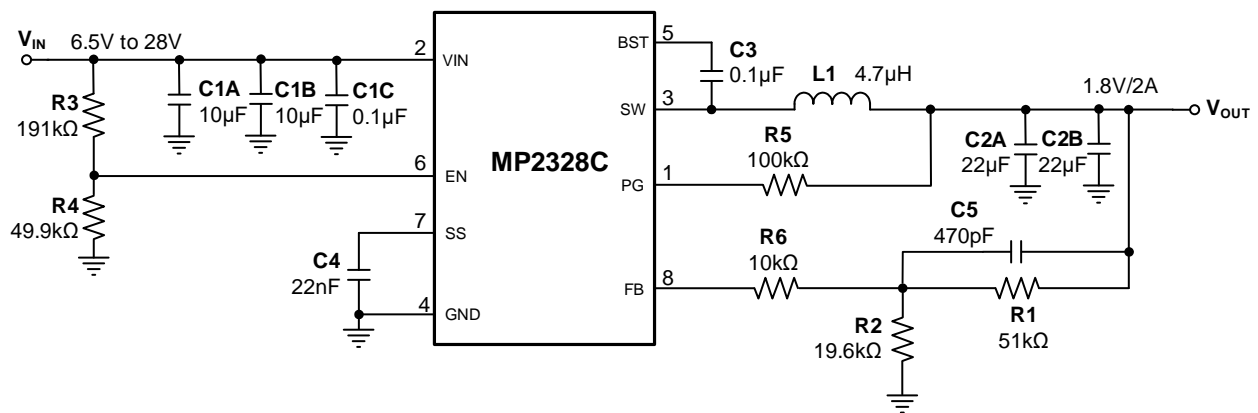
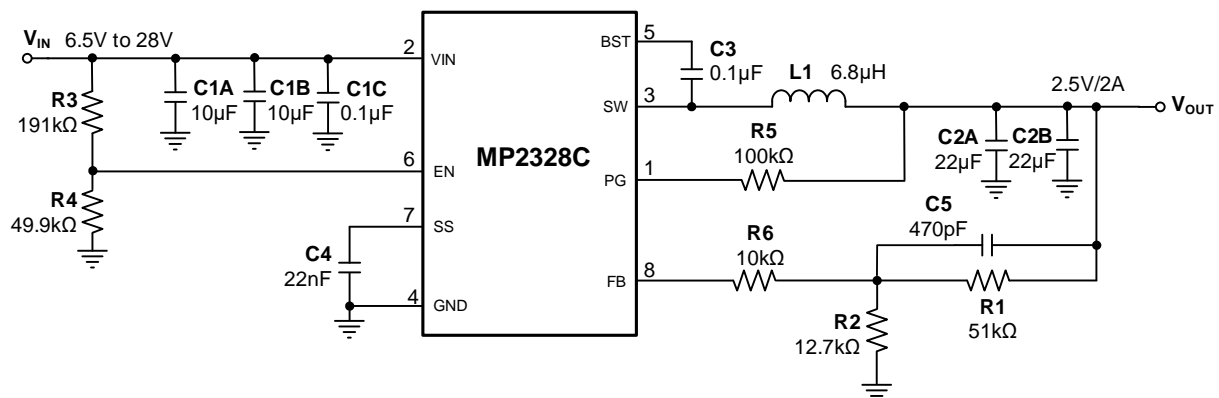
### PCB Layout Guidelines

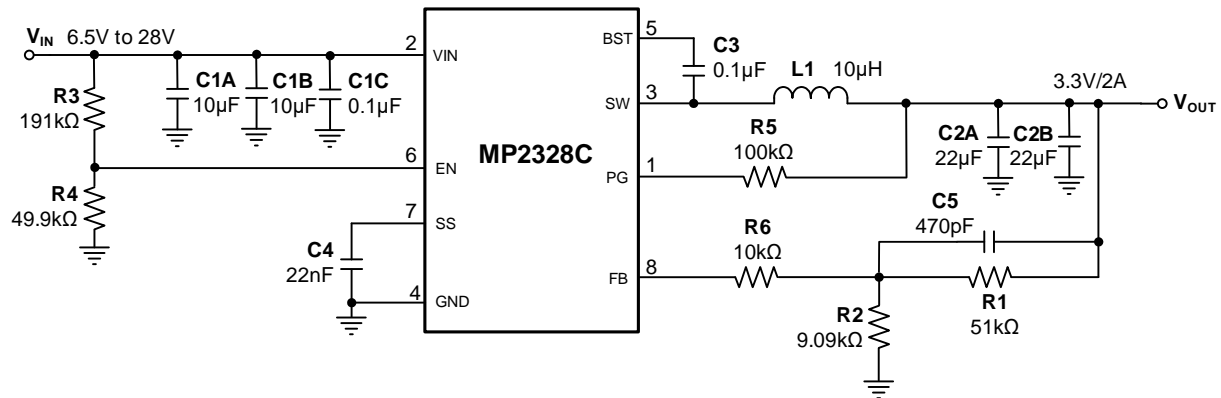
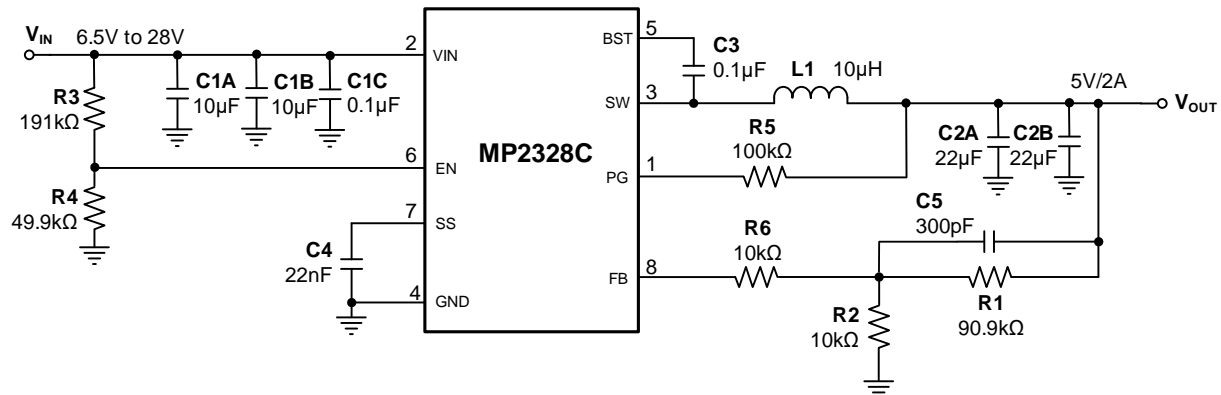
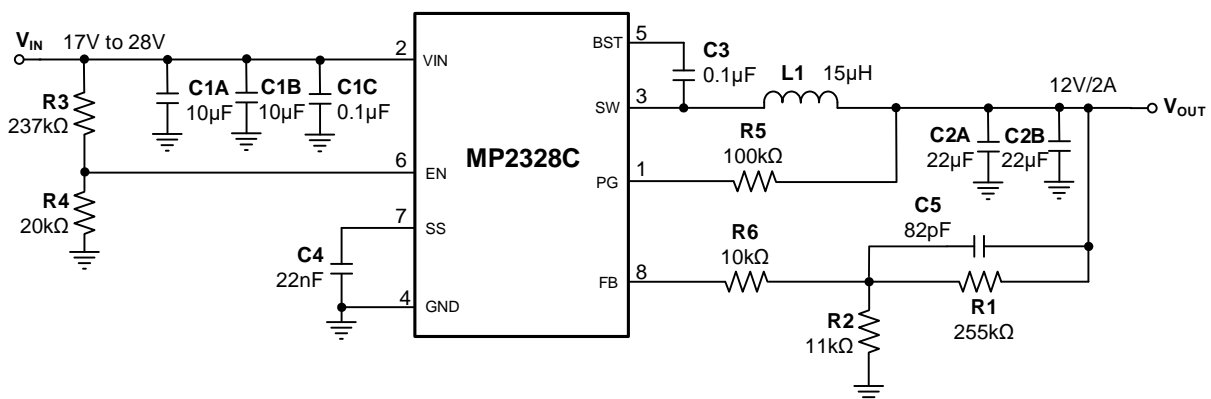
Proper layout of the switching power supplies is important for proper function. Poor layout design can result in poor line or load regulation and stability issues. For the best results, refer to Figure 4 and follow the guidelines below:

1. Place the high-current paths (GND, VIN, and SW) as close to the device as possible with short, direct, and wide traces.
2. Place the input capacitor as close to VIN and GND as possible (it is recommended to be within 1mm).
3. Place the external feedback resistors next to FB.
4. Keep the switching node (SW) short, and route it away from the feedback network.



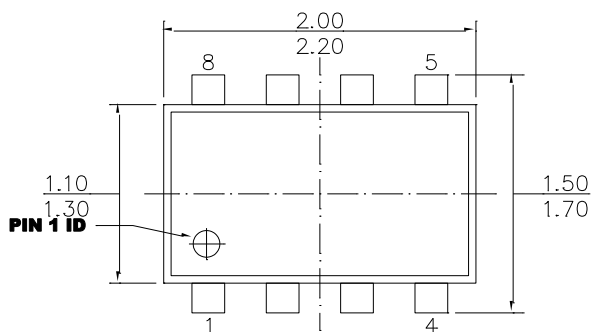
**Figure 4: Recommended PCB Layout**

**TYPICAL APPLICATION CIRCUITS**

**Figure 5: Typical Application Circuit ( $V_{IN} = 6.5V$  to  $28V$ ,  $V_{OUT} = 1V$ ,  $I_{OUT} = 2A$ )**

**Figure 6: Typical Application Circuit ( $V_{IN} = 6.5V$  to  $28V$ ,  $V_{OUT} = 1.8V$ ,  $I_{OUT} = 2A$ )**

**Figure 7: Typical Application Circuit ( $V_{IN} = 6.5V$  to  $28V$ ,  $V_{OUT} = 2.5V$ ,  $I_{OUT} = 2A$ )**

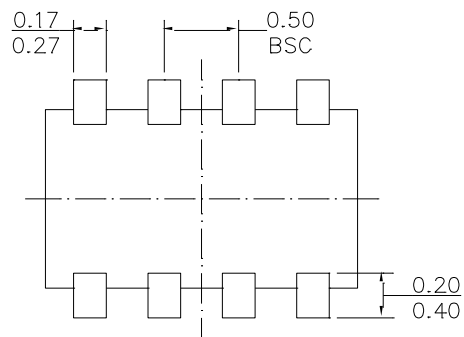
**TYPICAL APPLICATION CIRCUITS (continued)**

**Figure 8: Typical Application Circuit ( $V_{IN} = 6.5V$  to  $28V$ ,  $V_{OUT} = 3.3V$ ,  $I_{OUT} = 2A$ )**

**Figure 9: Typical Application Circuit ( $V_{IN} = 6.5V$  to  $28V$ ,  $V_{OUT} = 5V$ ,  $I_{OUT} = 2A$ )**

**Figure 10: Typical Application Circuit ( $V_{IN} = 17V$  to  $28V$ ,  $V_{OUT} = 12V$ ,  $I_{OUT} = 2A$ )**

# PACKAGE INFORMATION

## SOT583



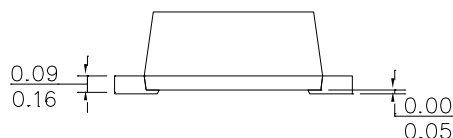
**TOP VIEW**



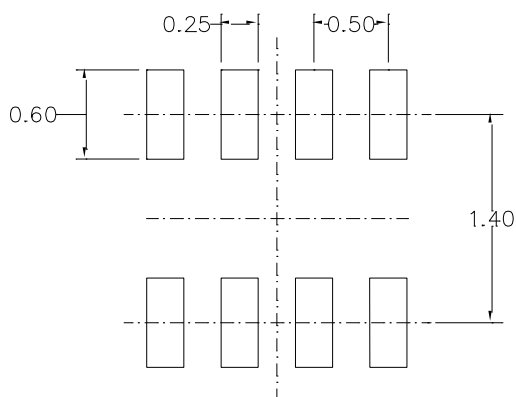
**BOTTOM VIEW**



**FRONT VIEW**



**SIDE VIEW**

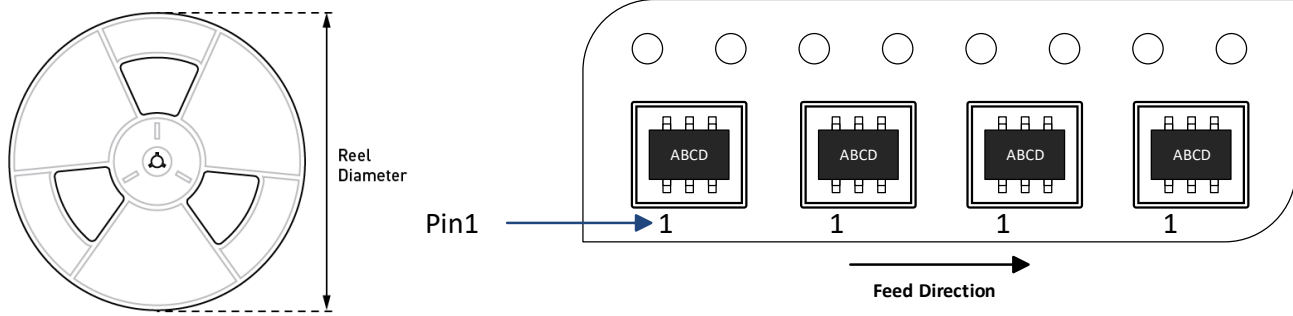


**RECOMMENDED LAND PATTERN**

**NOTE:**

- 1) ALL DIMENSIONS ARE IN MILLIMETERS.
- 2) PACKAGE WIDTH DOES NOT INCLUDE INTERLEAD FLASH OR PROTRUSION.
- 3) LEAD COPLANARITY (BOTTOM OF LEADS AFTER FORMING) SHALL BE 0.10 MILLIMETERS MAX.
- 4) DRAWING IS NOT TO SCALE.

### CARRIER INFORMATION



Part Number	Package Description	Quantity /Reel	Quantity/ Tube	Quantity/ Tube	Reel Diameter	Carrier Tape Width	Carrier Tape Pitch
MP2328CGTL-Z	SOT583	5000	N/A	N/A	7in	8mm	4mm

## REVISION HISTORY

Revision #	Revision Date	Description	Pages Updated
1.0	1/3/2022	Initial Release	-

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